

### General Description

The SM8001 high efficiency 1.5MHz synchronous buck converter operates over a wide input voltage range of 2.5V to 5.5V, and can deliver an output current up to 1A. It integrates a top MOSFET and a bottom MOSFET with very low  $R_{DS(ON)}$  to minimize conduction loss. The 1.5MHz pseudo-constant switching frequency enables using small external inductor and capacitor values.

The SM8001 uses constant-off time and peak current mode control strategy to achieve fast transient response and high efficiency at light loads. It also provides cycle-by-cycle current limit protection, output under voltage protection and over temperature protection.

Only the input and output capacitors, inductor, feedback resistor divider and feedforward capacitor need to be selected for the targeted application specifications.

### Features

- Low  $R_{DS(ON)}$  for Internal MOSFETs: 312mΩ Top, 192mΩ Bottom
- Wide Input Voltage Range: 2.5V ~ 5.5V
- Up to 1A Output Current
- $\pm 1.5\%$  0.6V Reference
- PFM Light Load Operation for High Efficiency
- Internal Soft-Start Limits the Inrush Current
- 1.5MHz Switching Frequency Minimizes the External Components
- Constant Off-time and Peak Current Mode Control to Achieve Fast Transient Responses
- 100% Dropout Operation
- Output Auto Discharge Function
- Cycle-by-Cycle Peak Current Limit Protection
- Hic-Cup Mode Output Under Voltage Protection
- Auto-Recovery Mode Over Temperature Protection
- Input Under Voltage Lockout (UVLO)
- RoHS-Compliant and Halogen-Free
- Compact Package: SOT23-5

### Applications

- Set-Top Box
- USB Dongle
- Media Player
- Smart Phone

### Typical Application

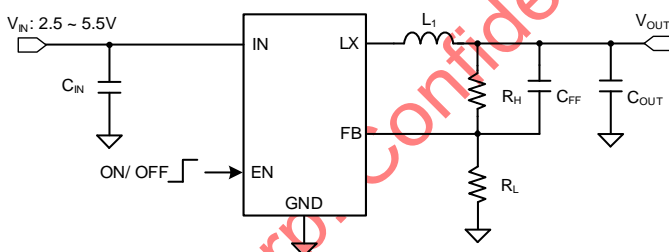


Figure 1. Schematic Diagram

Inductor and  $C_{OUT}$  Selection Table

$V_{OUT}[V]$	$L[\mu H]$	$C_{OUT}[\mu F]$			
		10	22	32	44
0.9	1.0		☆	√	√
	2.2	√	√	√	√
1.8	1.0	√	√	√	√
	2.2	√	☆	√	√
2.5/3.3	1.0	√	√	☆	√
	2.2	√	☆	√	√

Note: '☆' means recommended for most applications.

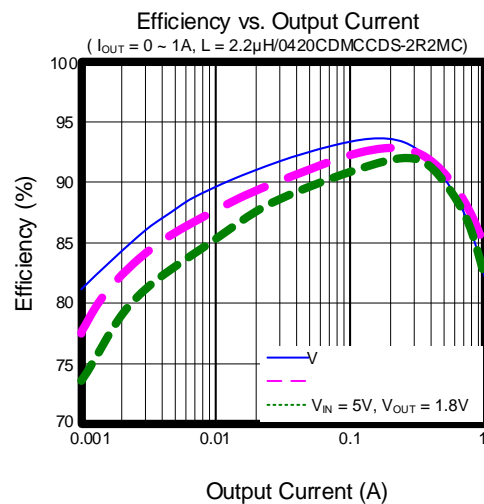


Figure 2. Efficiency vs. Output Current

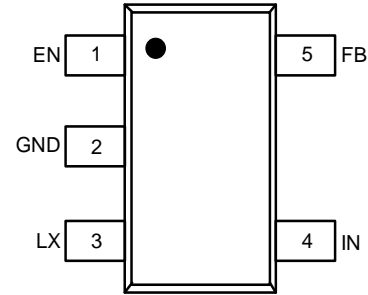


Ordering Information

Ordering Part Number	Package type	Top Mark
SM8001AAX	SOT23-5 RoHS Compliant and Halogen Free	KPW <sub>xyz</sub>

*x = year code, y = week code, z = lot number code*

Pinout (top view)



Pin Description

Pin No	Pin Name	Pin Description
1	EN	Enable pin. Pull this pin high to turn on the device and pull this pin low to turn off the device. Do not leave this pin floating.
2	GND	Ground pin.
3	LX	Inductor pin. Connect this pin to the switching node of inductor.
4	IN	Input pin. Decouple this pin from the GND pin with at least a 10μF ceramic capacitor.
5	FB	Output feedback pin. Connect this pin to the center point of the output resistor divider as shown in Figure 1. $V_{OUT} = 0.6 \times (1 + R_H/R_L)$ .



Block Diagram

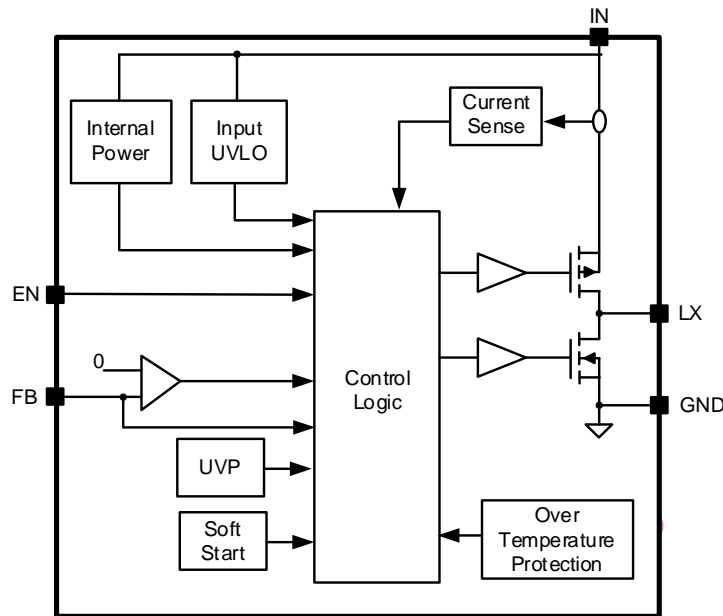


Figure3. Block Diagram

Absolute Maximum Ratings

Parameter (Note 1)	Min	Max	Unit
IN, LX	-0.3	6.5	V
EN, FB	-0.3	IN + 0.6	
LX, 40ns duration	-3	7	
Junction Temperature, Operating	-40	150	°C
Lead Temperature (Soldering, 10s)		260	
Storage Temperature	-65	150	

Thermal Information

Parameter (Note 2)	Typ	Unit
$\theta_{JA}$ Junction-to-Ambient Thermal Resistance	130	°C/W
$\theta_{JC}$ Junction-to-Case Thermal Resistance	28	
$P_D$ Power Dissipation $T_A = 25^\circ\text{C}$	0.77	W

Recommended Operating Conditions

Parameter (Note 3)	Min	Max	Unit
Input Voltage	2.5	5.5	V
Output Voltage	0.6	5.5	
Continuous Output Current		1	A
Ambient Temperature	-40	85	°C
Junction Temperature	-40	125	

**Electrical Characteristics**
 $(V_{IN} = 5V, V_{OUT} = 1.8V, L = 2.2\mu H, C_{OUT} = 10\mu F, T_J = 25^\circ C, I_{OUT} = 0.5A$  unless otherwise specified (Note 4))

Parameter	Symbol	Test Conditions	Min	Typ	Max	Unit
Input	Voltage Range	$V_{IN}$	2.5		5.5	V
	UVLO Rising Threshold	$V_{IN,UVLO}$			2.5	
	UVLO Hysteresis	$V_{IN,HYS}$		0.15		
	Quiescent Current	$I_Q$	$I_{OUT} = 0A, V_{FB} = V_{REF} \times 105\%$	50	60	$\mu A$
	Shutdown Current	$I_{SHDN}$	$V_{EN} = 0V$	0.1	1	
Output	Voltage Range	$V_{SET}$	0.6		5.5	V
	FB Reference Voltage	$V_{REF}$	0.591	0.6	0.609	
	Turn On Delay Time	$t_{ON,DLY}$	From EN high to LX starts switching		0.3	ms
	Soft-Start Time	$t_{SS}$	$V_{OUT}$ from 0% to 100% $V_{SET}$		0.7	
	Discharge on Resistance	$R_{DIS}$		50		
	UVP Threshold	$V_{UVP}$	(Note 5)		50	$\%V_{REF}$
	UVP Hiccup On-Time	$t_{HICCUP,ON}$	(Note 5)		1.6	ms
	UVP Hiccup Off-Time	$t_{HICCUP,OFF}$	(Note 5)		1.6	
Enable (EN)	Input Voltage High	$V_{EN,H}$	1			V
	Input Voltage Low	$V_{EN,L}$			0.4	
MOSFET	Top MOSFET $R_{DS(ON)}$	$R_{DS(ON),TOP}$	216	312	408	m $\Omega$
	Bottom MOSFET $R_{DS(ON)}$	$R_{DS(ON),BOT}$	120	192	264	
	Top MOSFET Current Limit Threshold	$I_{LMT,TOP}$		1.5	2.5	A
Frequency	Switching Frequency	$f_{SW}$	$I_{OUT} = 0.5A, CCM$	1.5		MHz
	Minimum On-Time	$t_{ON,MIN}$	(Note 5)	50		ns
	Maximum Duty Cycle	$D_{MAX}$	(Note 5)	100		%
OTP	Temperature	$T_{OTP}$	(Note 5)	160		$^\circ C$
	Temperature Hysteresis	$T_{HYS}$	(Note 5)	20		

**Note 1:** Stresses beyond the “Absolute Maximum Ratings” may cause permanent damage to the device. These are stress ratings only. Functional operation of the device at these or any other conditions beyond those indicated in the operational sections of the specification is not implied. Exposure to absolute maximum rating conditions for extended periods may affect device reliability.

**Note 2:**  $\theta_{JA}$  is measured in the natural convection at  $T_A = 25^\circ C$  on a 6cmx6cm size, two-layer Silergy Evaluation Board with 2-oz copper. Pin 3 of SOT23-5 package is the case position for  $\theta_{JC}$  measurement.

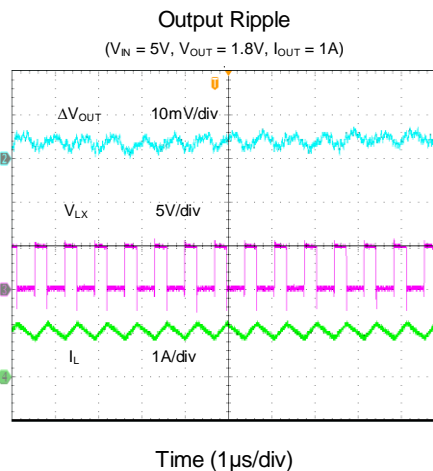
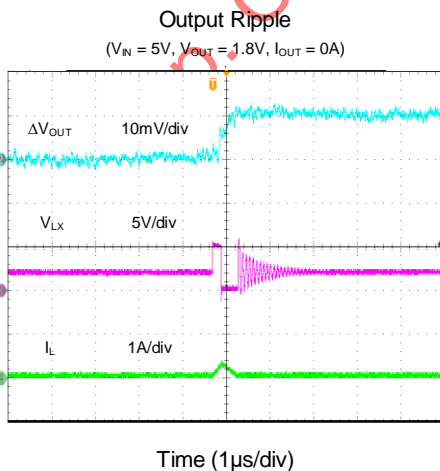
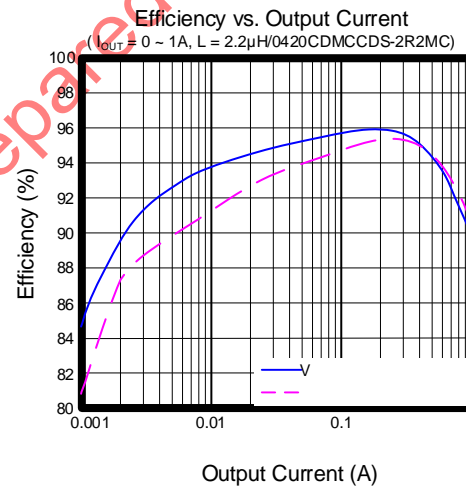
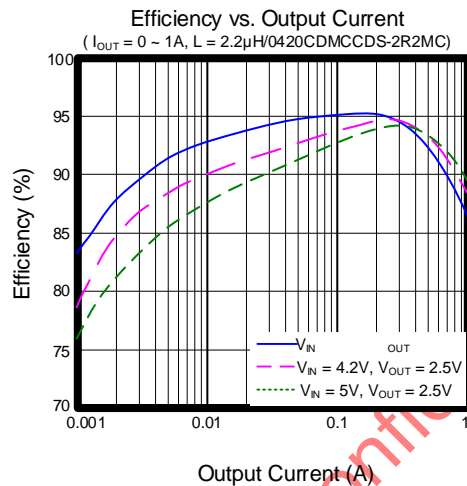
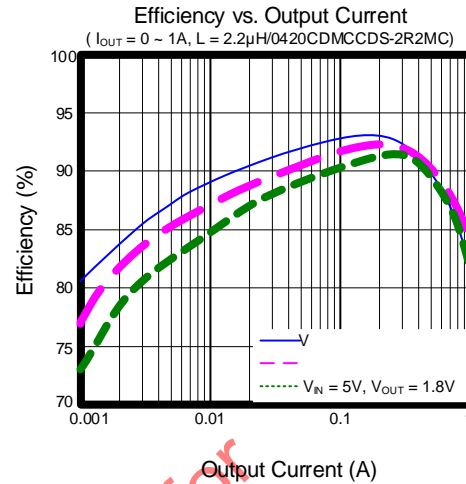
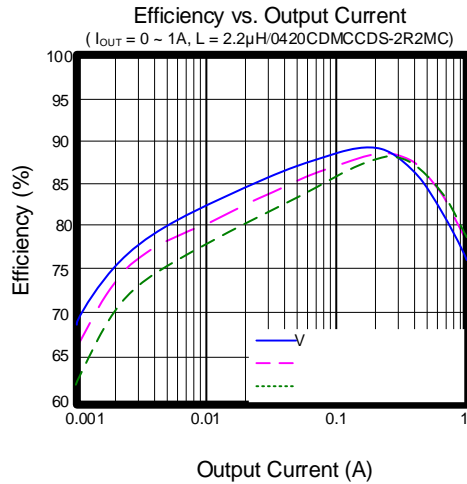
**Note 3:** The device is not guaranteed to function outside its operating conditions.

**Note 4:** Unless otherwise stated, limits are 100% production tested under pulsed load conditions such that  $T_A \cong T_J = 25^\circ C$ . Limits over the operating temperature range (See recommended operating conditions) and relevant voltage range(s) are guaranteed by design, test, or statistical correlation.

**Note 5:** Guaranteed by design or statistical correlation and not production tested.

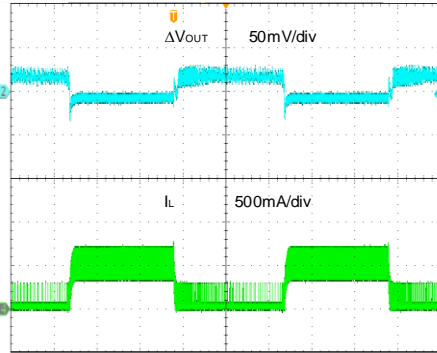
## Typical Performance Characteristics

( $T_A = 25^\circ\text{C}$ ,  $V_{IN} = 5\text{V}$ ,  $V_{OUT} = 1.8\text{V}$ ,  $L = 2.2\mu\text{H}$ ,  $C_{OUT} = 10\mu\text{F}$ , unless otherwise noted)



Load Transient

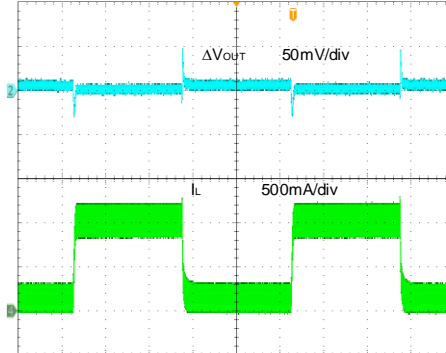
( $V_{IN} = 5V$ ,  $V_{OUT} = 1.8V$ ,  $I_{OUT} = 0A \sim 0.5A$ )



Time (400 $\mu$ s/div)

Load Transient

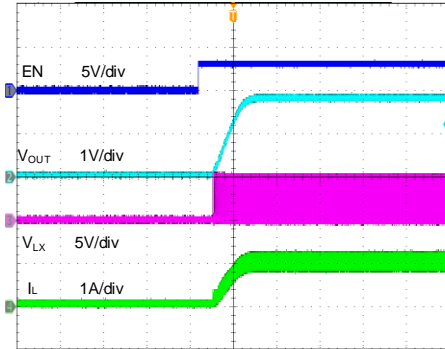
( $V_{IN} = 5V$ ,  $V_{OUT} = 1.8V$ ,  $I_{OUT} = 0.1A \sim 1A$ )



Time (400 $\mu$ s/div)

Startup from Enable

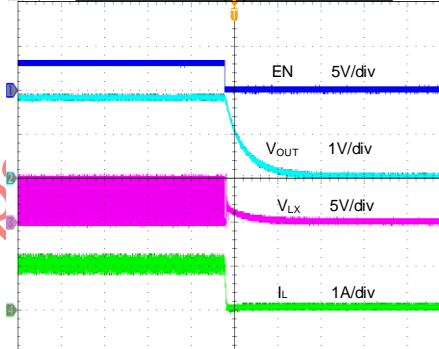
( $V_{IN} = 5V$ ,  $V_{OUT} = 1.8V$ ,  $I_{OUT} = 1A$ )



Time (800 $\mu$ s/div)

Shutdown from Enable

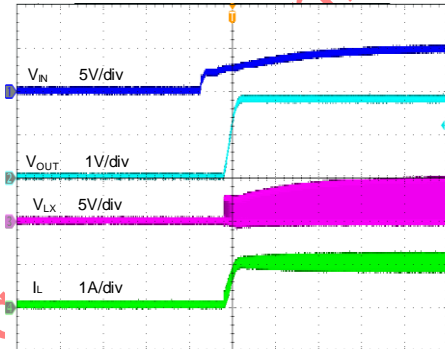
( $V_{IN} = 5V$ ,  $V_{OUT} = 1.8V$ ,  $I_{OUT} = 1A$ )



Time (40 $\mu$ s/div)

Startup from  $V_{IN}$

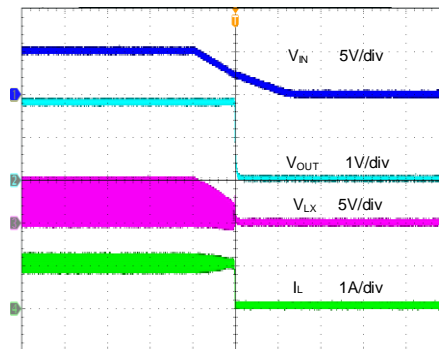
( $V_{IN} = 5V$ ,  $V_{OUT} = 1.8V$ ,  $I_{OUT} = 1A$ )



Time (2ms/div)

Shutdown from  $V_{IN}$

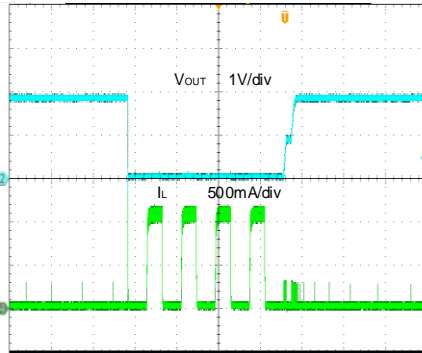
( $V_{IN} = 5V$ ,  $V_{OUT} = 1.8V$ ,  $I_{OUT} = 1A$ )



Time (800 $\mu$ s/div)

### Short Circuit Protection

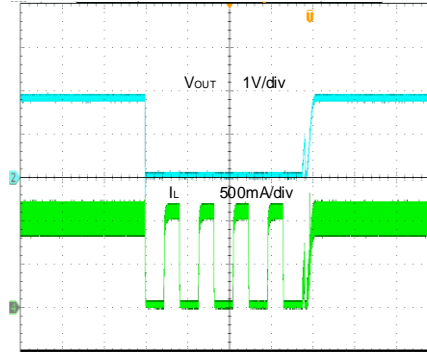
( $V_{IN} = 5V$ ,  $V_{OUT} = 1.8V$ ,  $I_{OUT} = 0A \sim \text{short}$ )



Time (4ms/div)

### Short Circuit Protection

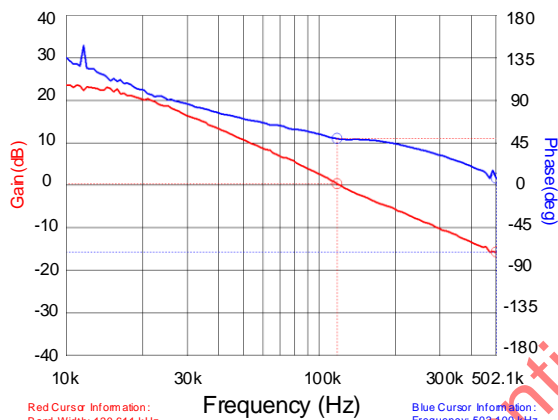
( $V_{IN} = 5V$ ,  $V_{OUT} = 1.8V$ ,  $I_{OUT} = 1A \sim \text{short}$ )



Time (4ms/div)

### Bode Plot

( $V_{IN} = 5V$ ,  $V_{OUT} = 0.9V$ ,  $I_{OUT} = 1A$ )

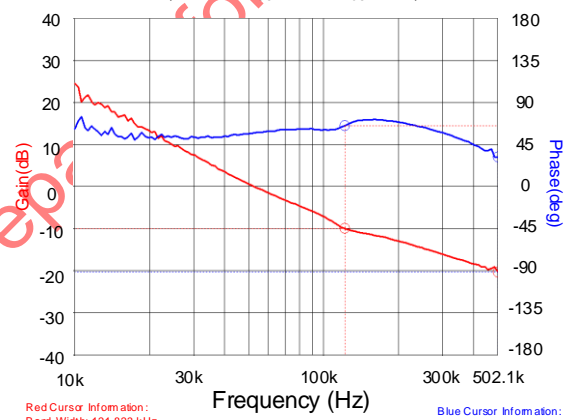


Red Cursor Information:  
Band Width: 120.611 kHz  
Phase Margin: 48.919 deg

Blue Cursor Information:  
Frequency: 502.100 kHz  
Gain: -15.732 dB

### Bode Plot

( $V_{IN} = 5V$ ,  $V_{OUT} = 1.8V$ ,  $I_{OUT} = 1A$ )

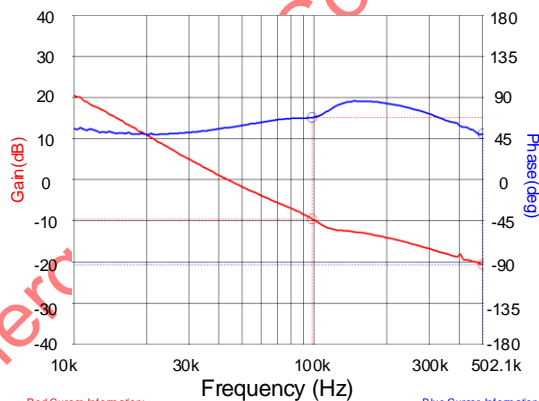


Red Cursor Information:  
Band Width: 121.823 kHz  
Phase Margin: 65.119 deg

Blue Cursor Information:  
Frequency: 502.1 kHz  
Gain: -10.311 dB

### Bode Plot

( $V_{IN} = 5V$ ,  $V_{OUT} = 2.5V$ ,  $I_{OUT} = 1A$ )

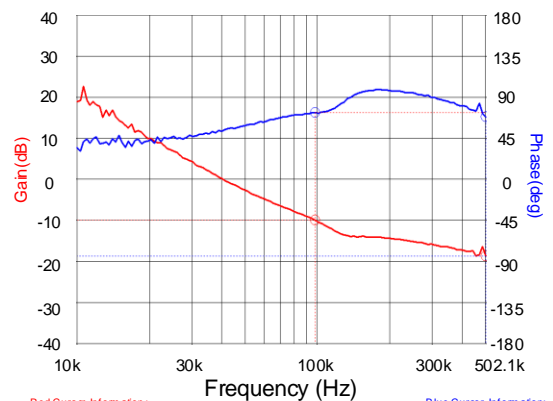


Red Cursor Information:  
Band Width: 101.007 kHz  
Phase Margin: 68.845 deg

Blue Cursor Information:  
Frequency: 502.100 kHz  
Gain: -10.620 dB

### Bode Plot

( $V_{IN} = 5V$ ,  $V_{OUT} = 3.3V$ ,  $I_{OUT} = 1A$ )



Red Cursor Information:  
Band Width: 98.493 kHz  
Phase Margin: 72.886 deg

Blue Cursor Information:  
Frequency: 502.100 kHz  
Gain: -8.684 dB

## Detailed Description

### General Description

The SM8001 high efficiency 1.5MHz synchronous buck converter operates over a wide input voltage range of 2.5V to 5.5V, and can deliver an output current up to 1A. It integrates a top MOSFET and a bottom MOSFET with very low  $R_{DS(ON)}$  to minimize conduction loss. The 1.5MHz pseudo-constant switching frequency allows small external inductor and capacitor values.

The SM8001 also provides cycle-by-cycle current limit protection output under voltage protection and over temperature protection.

### Constant Off-Time and Peak Current Mode Control

The device uses instant PWM architecture to achieve fast transient response and high efficiency at light loads. It uses a constant off-time and peak current mode control strategy. When the top MOSFET's current-sense signal reaches internal  $V_{COMP}$ , the top MOSFET turns off and the bottom MOSFET turns on for a fixed period of time (constant  $t_{OFF}$ ).  $t_{OFF}$  is internally calculated according to the input voltage, output voltage, and desired switching frequency ( $f_{SW}$ ):

$$t_{OFF} = \frac{1 - V_{OUT}/V_{IN}}{f_{SW}}$$

The bottom MOSFET turns off after a period of  $t_{OFF}$ .

### Minimum and Maximum Duty Cycle

There is minimum on-time limitation in the constant off-time architecture. The device supports low to 10% duty cycle application across the entire operating temperature range of  $-40^{\circ}\text{C} \sim 125^{\circ}\text{C}$ .

The device can support a maximum duty cycle of up to 100% across the entire operating temperature range of  $-40^{\circ}\text{C} \sim 125^{\circ}\text{C}$ .

### PFM Light Load Operation

The device uses pulse-frequency modulation (PFM) operation mode under light load condition for high efficiency. Under light load conditions, typically when the load satisfies the following equation,

$$I_{OUT\_CTL} = \frac{\Delta I_L}{2} = \frac{V_{OUT} \times (1 - D)}{2 \times f_{SW} \times L}$$

the current through the bottom MOSFET will ramp to near zero before the next  $t_{ON}$  time. When this occurs, the bottom MOSFET turns off, preventing recirculation current that can seriously reduce efficiency under these light load conditions. As load current is further reduced, the combined feedback and ramp signals remain much higher than the reference voltage, the instant-PWM control loop will not trigger another  $t_{ON}$  until needed, and the apparent operating switching frequency will correspondingly drop, improving efficiency. Continuous conduction mode (CCM) resumes

smoothly as soon as the load current increases sufficiently for the inductor current to remain above zero at the time of the next  $t_{ON}$  cycle. The buck converter enters CCM once the load current exceeds the threshold shown in (1). Above the threshold, the switching frequency stays fairly constant over the output current range.

While in PFM mode, the output of the device doesn't require over voltage protection because the device stops switching as soon as the voltage at the FB node increases above  $V_{REF}$ , preventing the output voltage from increasing further.

### Input Under Voltage Lockout (UVLO)

To prevent operation before the internal circuitry is ready and to ensure that the top and bottom MOSFETs can be properly driven, the device incorporates an input under voltage lockout protection. The device remains in a low current state and all LX node switching actions are inhibited until  $V_{IN}$  exceeds its rising threshold. At that time, if EN is enabled, the device will startup. If  $V_{IN}$  falls below  $V_{IN,UVLO}$  less than the input UVLO hysteresis, the LX node switching actions will again be suppressed.

### Enable Control

The EN input is a high-voltage input with logic-compatible threshold. When EN is driven above 1V, normal device operation is enabled. When EN is driven to less than 0.4V, the device will shut down, reducing the input current to less than  $1\mu\text{A}$ .

It is not recommended to connect EN pin directly to  $V_{IN}$  or another voltage source. A resistor in a range of  $1\text{k}\Omega$  to  $1\text{M}\Omega$  should be used if EN pin is pulled high.

### Soft-Start

The device incorporates an internal soft-start circuit to ramp the output to the desired voltage whenever the device is enabled. Internally, the soft-start circuit clamps the output at a low voltage and then allows the output to rise to the desired voltage over approximately 0.7ms, which avoids high current flow and transients during startup.

## Fault Protection Modes

### Cycle-by-Cycle Current Limit Protection

If the top MOSFET current exceeds the top current limit threshold, it will turn off and the bottom MOSFET will turn on. As a result, inductor peak current is limited.

### Output Under Voltage Protection (UVP)

With output current increasing, the top MOSFET current will exceed its current limit threshold, and if the load current continues to increase, the output voltage will drop. When the output voltage falls below 50% of the regulated level, the output under voltage protection will be activated and the device will operate in hiccup mode. The hiccup on-time is 1.6ms, and the hiccup off-time is 1.6ms. If the hard short

condition is removed, the device will return to normal operation.

### Over Temperature Protection (OTP)

The device includes over temperature protection (OTP) circuitry to prevent overheating due to excessive power dissipation. This will shut down the device when the junction temperature exceeds 160°C. When the junction temperature is reduced by approximately 20°C, the device will resume normal operation after a complete soft-start cycle. For continuous operation, provide adequate thermal dissipation so that the junction temperature does not exceed the OTP threshold.

## Application Information

The following paragraphs provide information on the selection of the external components needed to meet the targeted application specifications.

### Feedback Resistor Divider $R_H$ and $R_L$

Choose  $R_H$  and  $R_L$  to program the proper output voltage. A value between 1kΩ and 1MΩ is recommended for both resistors to minimize power consumption under light loads. As an example, if  $V_{OUT} = 1.8V$  and  $R_H$  selected value is 100kΩ,  $R_L$  can be calculated as follows:

$$R_L = \frac{0.6}{V_{OUT} - 0.6V} \times R_H$$

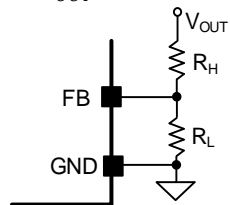


Figure4. Feedback Resistor Divider

With a calculated value of 50kΩ for  $R_L$ , a standard 1% 49.9kΩ resistor is selected.

### Input Capacitor $C_{IN}$

For the best performance, select a typical X5R or better grade ceramic capacitor with a 10V rating, and at least 10μF capacitance. The capacitor should be placed as close as possible to the device, while also minimizing the loop area formed by  $C_{IN}$  and the IN/GND pins.

When selecting an input capacitor, ensure that its voltage rating is at least 20% greater than the maximum voltage of the input supply. X5R or X7R dielectric types are the most often selected due to their small size, low cost, surge current capability, and high RMS current rating over a wide temperature and voltage range.

In situations where the input rail is supplied through long wires, it is recommended to add some bulk capacitance like

electrolytic, tantalum or polymer type capacitors to reduce the overshoot and ringing caused by the added parasitic inductance.

Consider the RMS current rating of the input capacitor, paralleling additional capacitors if required to meet the calculated RMS ripple current.

$$I_{CIN\_RMS} = I_{OUT} \times \sqrt{D \times (1 - D)}$$

The worst-case condition occurs at  $D = 0.5$ , then

$$I_{CIN\_RMS\_MAX} = \frac{I_{OUT}}{2}$$

For simplicity, use an input capacitor with an RMS current rating greater than 50% of the maximum load current. The input capacitor value determines the input voltage ripple of the converter. If there is a voltage ripple requirement in the system, choose an appropriate input capacitor that meets the specification.

Given the very low ESR and ESL of ceramic capacitors, the input voltage ripple can be estimated using the formula:

$$V_{CIN\_RIPPLE,CAP} = \frac{I_{OUT}}{f_{SW} \times C_{IN}} \times D \times (1 - D)$$

The worst-case condition occurs at  $D = 0.5$ , then

$$V_{CIN\_RIPPLE,CAP\_MAX} = \frac{I_{OUT}}{4 \times f_{SW} \times C_{IN}}$$

The capacitance value is less important than the RMS current rating. A single 10μF X5R capacitor is sufficient for most applications.

### Output Inductor L

Consider the following when choosing this inductor:

- 1) Choose the inductance to provide a ripple current that is approximately 40% of the maximum output current. The recommended inductance is calculated as:

$$L = \frac{V_{OUT}(1 - V_{OUT}/V_{IN,MAX})}{f_{sw} \times I_{OUT,MAX} \times 0.4}$$

where  $f_{sw}$  is the switching frequency and  $I_{OUT,MAX}$  is the maximum load current.

The device has high tolerance for ripple current amplitude variation. As a result, the final choice of inductance can vary slightly from the calculated value with no significant performance impact.

- 2) The inductor's saturation current rating must be greater than the peak inductor current under full load:

$$I_{SAT,MIN} > I_{OUT,MAX} + \frac{V_{OUT}(1 - V_{OUT}/V_{IN,MAX})}{2 \times f_{SW} \times L}$$



- 3) The DCR of the inductor and the core loss at the switching frequency must be low enough to achieve the desired efficiency requirement. Use an inductor with DCR less than 50mΩ to achieve good overall efficiency.

**Output Capacitor C<sub>OUT</sub>**

Select the output capacitor C<sub>OUT</sub> to handle the output ripple requirements. Both steady state ripple and transient requirements must be taken into consideration when selecting C<sub>OUT</sub>. For the best performance, use a X5R or better grade ceramic capacitor with a 6.3V rating, and capacitance of at least 10μF.

For applications where the design must meet stringent ripple requirements, the following considerations must be followed.

The output voltage ripple at the switching frequency is caused by the inductor current ripple (ΔI<sub>L</sub>) on the output capacitor's ESR (ESR ripple), as well as the stored charge (capacitive ripple). When calculating total ripple, consider both.

$$V_{RIPPLE,ESR} = \Delta I_L \times ESR$$

$$V_{RIPPLE,CAP} = \frac{\Delta I_L}{8 \times C_{OUT} \times f_{SW}}$$

The measured capacitive ripple might be higher than the theoretical value because the effective capacitance for ceramic capacitors decreases with the voltage across its terminals. The voltage derating is usually included as a chart in the capacitor datasheet, and the ripple can be recalculated after taking the target output voltage into account.

**Feedforward Capacitor C<sub>FF</sub>**

The device integrates the compensation components to achieve good stability and fast transient responses. In some applications, adding a ceramic capacitor (feedforward capacitor C<sub>FF</sub>) in parallel with R<sub>H</sub> may further speed up the load transient response. Note that when the output LC parameter is large, the feedforward capacitor can be increased for providing sufficient ripple to FB for small output ripple and good transient behavior.

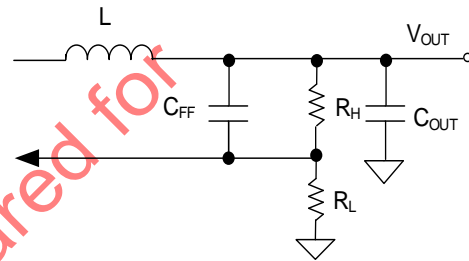


Figure5. Feedforward Network

## Application Schematic ( $V_{OUT} = 1.8V$ )

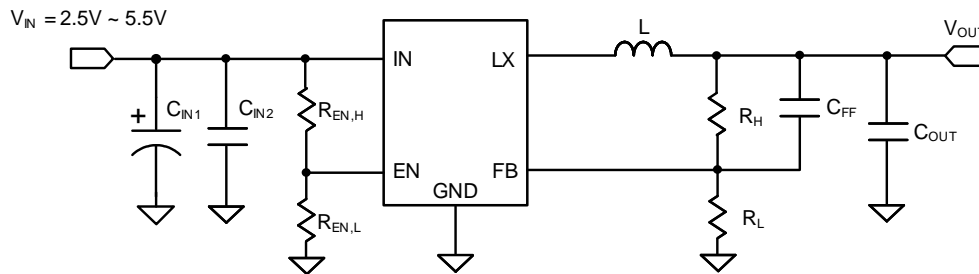


Figure6. Schematic Diagram

## BOM List

Reference Designator	Description	Part Number	Manufacturer
C <sub>IN1</sub>	47 $\mu$ F/50V Electrolytic Capacitor		
C <sub>IN2</sub>	10 $\mu$ F/10V/X5R, 0805	GRM21BR71A106KA73L	m $\mu$ Rata
C <sub>OUT</sub>	10 $\mu$ F/10V/X5R, 0805	GRM21BR71A106KA73L	m $\mu$ Rata
C <sub>FF</sub>	22pF/50V/C0G, 0603	GRM1885C1H220JA01D	m $\mu$ Rata
L	2.2 $\mu$ H/inductor	0420CDMCCDS-2R2MC	Sumida
R <sub>H</sub>	100k $\Omega$ , 1%, 0603		
R <sub>L</sub>	49.9k $\Omega$ , 1%, 0603		
R <sub>EN,H</sub>	10k $\Omega$ , 1%, 0603		
R <sub>EN,L</sub>	1M $\Omega$ , 1%, 0603		

## Recommend Component Values for Typical Applications

V <sub>OUT</sub> (V)	R <sub>H</sub> (k $\Omega$ )	R <sub>L</sub> (k $\Omega$ )	C <sub>FF</sub> (pF)	L/Part Number	C <sub>OUT</sub>
0.9	100	200	22	0420CDMCCDS-2R2MC	10 $\mu$ F/10V/X5R, 0805
1.8	100	49.9	22	0420CDMCCDS-2R2MC	10 $\mu$ F/10V/X5R, 0805
2.5	100	31.4	22	0420CDMCCDS-2R2MC	10 $\mu$ F/10V/X5R, 0805
3.3	100	22.1	22	0420CDMCCDS-2R2MC	10 $\mu$ F/10V/X5R, 0805

## Layout Design

Follow these PCB layout guidelines for optimal performance and thermal dissipation:

**Input Capacitor:** Place the input capacitor very close to IN and GND pins, minimizing the loop formed by these connections. The input capacitor should be connected to the IN and GND pins using a wide copper area.

**Output Capacitor:** Connect the  $C_{OUT}$  negative terminal to the GND pin using wide copper traces instead of vias, in order to achieve better accuracy and stability of the output voltage.

**Feedback Network:** Place the feedback components ( $R_H$ ,  $R_L$  and  $C_{FF}$ ) as close to the FB pin as possible. Avoid routing the feedback line near LX, or other high-frequency signals as it is noise-sensitive. Use a Kelvin connection to connect with  $C_{OUT}$  rather than the inductor output terminal.

**LX Connection:** Keep the LX area small to prevent excessive EMI, while providing a wide copper trace to minimize parasitic resistance and inductance.

**EN Signal:** It is **not** recommended to connect EN pin directly to  $V_{IN}$  or another voltage source. A resistor in a range of  $1k\Omega$  to  $1M\Omega$  should be used if EN pin is pulled high.

**GND Vias:** Place an adequate number of vias on the GND layer around the device for better thermal performance.

**PCB Board:** To achieve the best thermal and noise performance, maximize the PCB copper area connecting to the GND pin. A ground plane is highly recommended if possible. Connect the ground pad to a large copper area to enhance thermal performance.

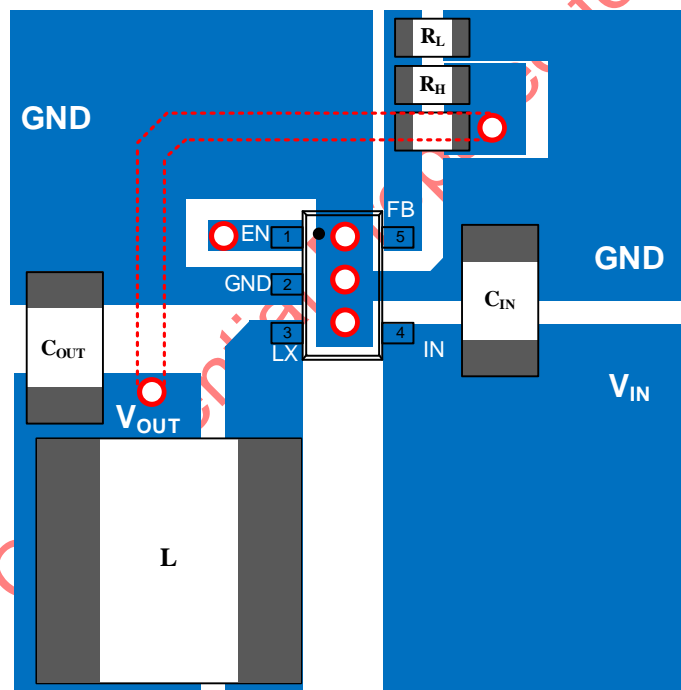
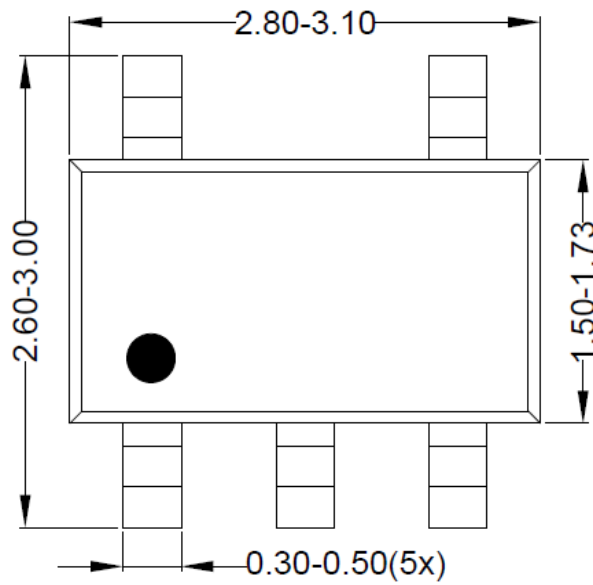
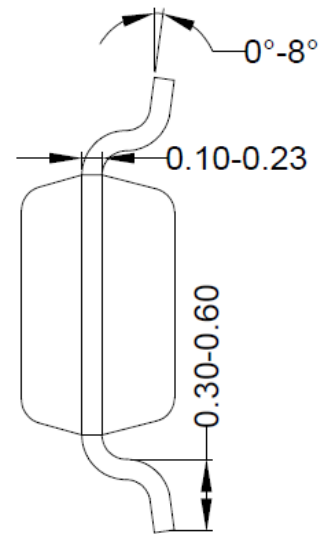


Figure7. Suggested PCB Layout

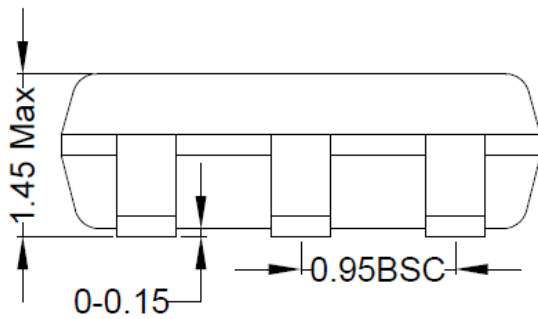
**SOT23-5 Package Outline & PCB layout**



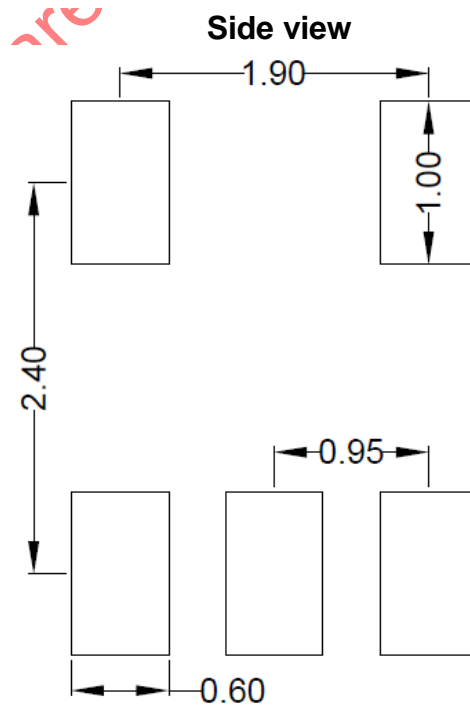
**Top view**



**Side view**



**Front view**



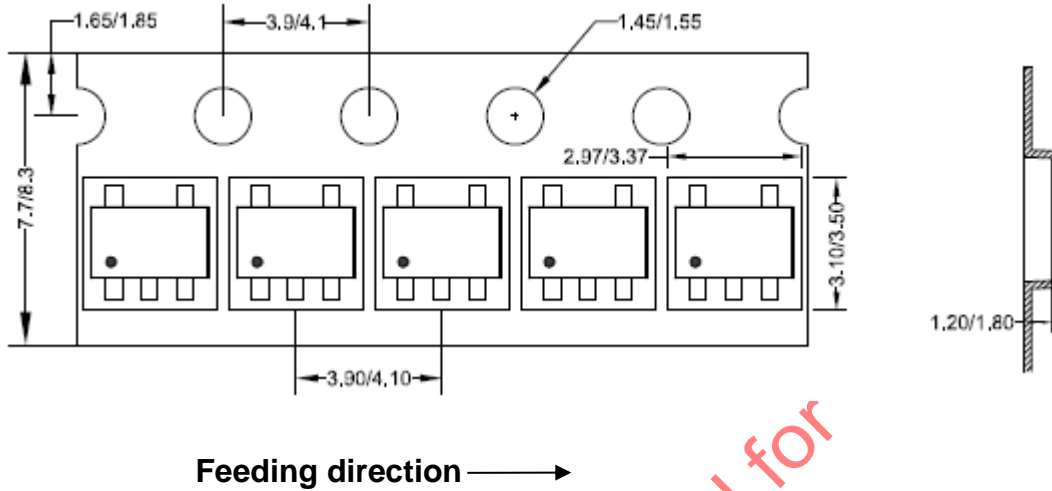
**Recommended PCB pad Layout  
(Reference only)**

**Notes:** All dimension in millimeter and exclude mold flash & metal burr.

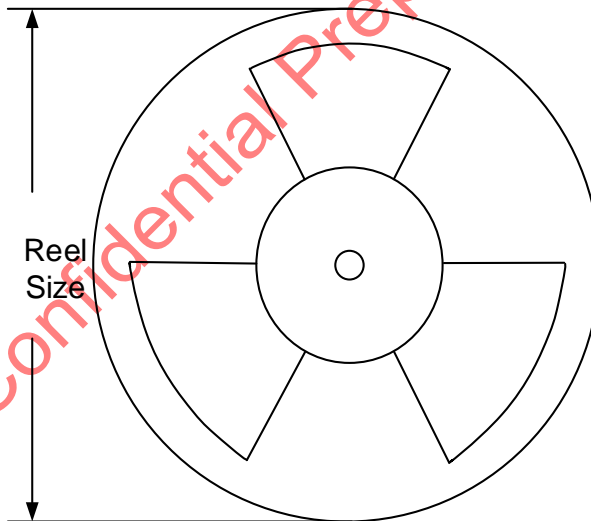
**Tape and Reel Specification**

**1. Tape orientation**

**SOT23-5**



**2. Carrier Tape and Reel specification for packages**



Package type	Tape width (mm)	Pocket pitch(mm)	Reel size (Inch)	Trailer length(mm)	Leader length (mm)	Qty per reel
SOT23-5	8	4	7	280	160	3000

## Revision History

The revision history provided is for informational purpose only and is believed to be accurate, however, not warranted. Please make sure that you have the latest revision.

Date	Revision	Change	Pages changed
Dec. 4, 2024	1.0	Initial Release.	-

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